

IS32LT3953B

CONSTANT-CURRENT 3-AMPERE PWM DIMMABLE BUCK REGULATOR LED DRIVER WITH FAULT PROTECTION

June 2020

GENERAL DESCRIPTION

The IS32LT3953B is a DC-to-DC switching converter that integrates an N-channel MOSFET to operate in a buck configuration. The device can operate from a wide input voltage between 4.5V and 38V and provides a constant current of up to 3A for driving a single LED or multiple series connected LEDs.

The external resistor, R_{SET} , is used to set a constant LED output current, while allowing the output voltage to be automatically adjusted for a variety of LED configurations.

The IS32LT3953B operates in a fixed frequency mode during switching. There is an external resistor connected between the VCC and TON pins used to configure the on-time (switching frequency). The switching frequency is dithered for spread spectrum operation which will spread the electromagnetic energy into a wider frequency band. This function is helpful for optimizing EMI performance.

A logic input PWM signal applied to the enable (EN) pin will adjust the average LED current. The LED brightness is proportional to the duty cycle of the PWM signal.

True average output current operation is achieved with fast transient response by using cycle-by-cycle, controlled on-time method.

The IS32LT3953B is available in an SOP-8-EP package with an exposed pad for enhanced thermal dissipation. It operates from 4.5V to 38V over the temperature range of -40°C to $+125^{\circ}\text{C}$.

FEATURES

- Wide input voltage supply from 4.5V to 38V
 - Withstand 40V load dump
- True average output current control
- 3A maximum output over operating temperature range
- Cycle-by-cycle current limit
- Integrated high-side MOSFET switch
- Dimming via analog input, direct logic input or power supply voltage
- Internal control loop compensation
- Under-voltage lockout (UVLO) and thermal shutdown protection
- 2 μA low power shutdown
- Spread spectrum to optimize EMI
- Internal linear regulator output (VDD) to bias the external circuit
- Robust fault protection:
 - Pin-to-GND short
 - Component open/short faults
 - Adjacent pin-to-pin short
 - LED open/short
 - Thermal shutdown
- AEC-Q100 Qualified

APPLICATIONS

- Automotive and avionic lighting
- Daytime running lights
- Turn/stop lights
- Front and rear fog lights
- Matrix headlight
- Motorcycle headlight

TYPICAL APPLICATION CIRCUIT

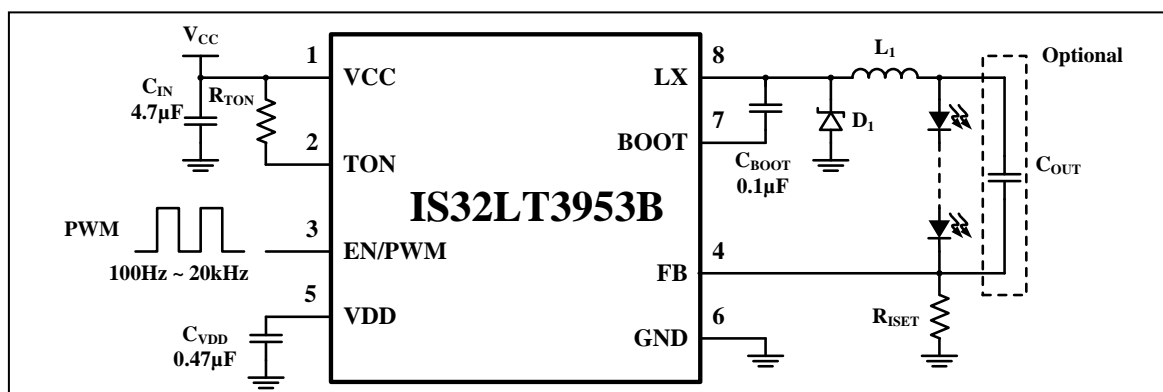


Figure 1 Typical Application Circuit

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TYPICAL APPLICATION CIRCUIT (CONTINUE)

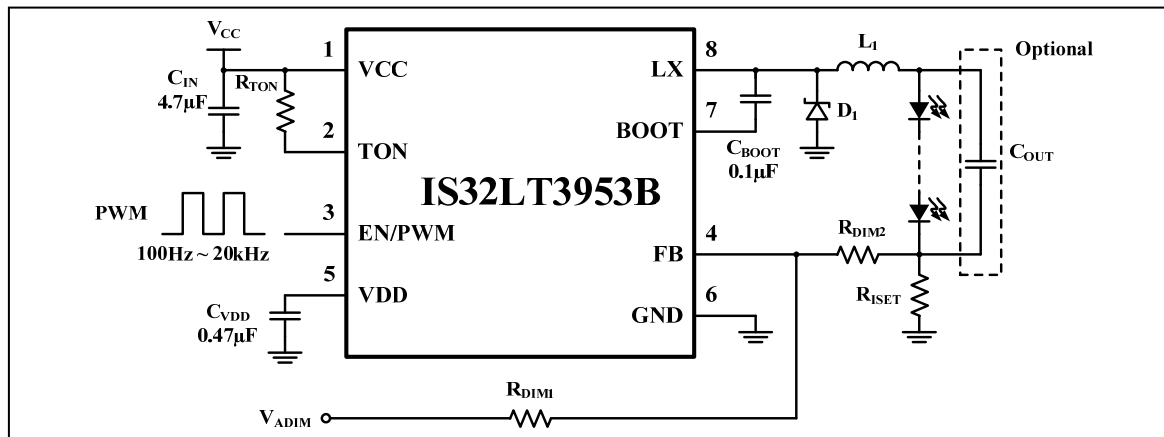


Figure 2 Typical Application Circuit of Analog Dimming

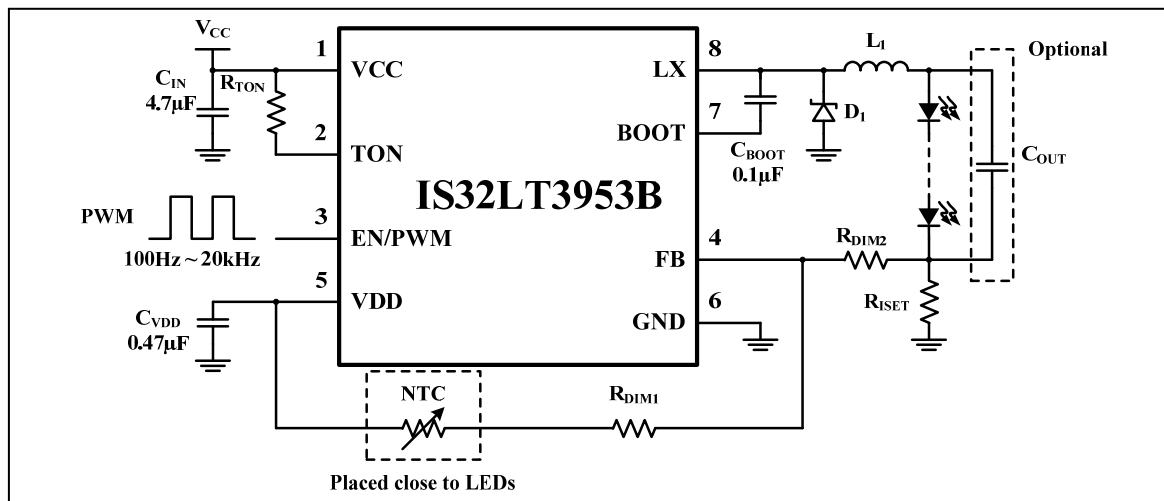
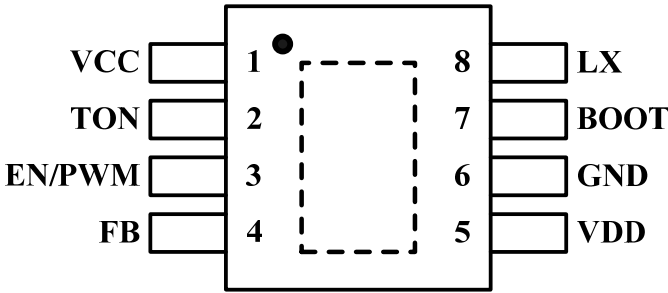


Figure 3 Typical Application Circuit Of Thermal Rolloff with External NTC

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PIN CONFIGURATION

Package	Pin Configuration (Top View)
SOP-8-EP	

PIN DESCRIPTION

No.	Pin	Description
1	VCC	Power supply input. Connect a bypass capacitor C_{IN} to ground. The path from C_{IN} to GND and VCC pins should be as short as possible.
2	TON	On-time setting. Connect a resistor from this pin to VCC pin to set the regulator controlled on-time.
3	EN/PWM	Logic input for enable and PWM dimming. Pull up above 1.4V to enable and below 0.4V to disable. Input a 100Hz~20kHz PWM signal to dim the LED brightness.
4	FB	Drive output current sense feedback. Set the output current by connecting a resistor from this pin to the ground.
5	VDD	Regulator output pin. Connect a 0.47 μ F X7R ceramic capacitor from this pin to GND.
6	GND	Ground. Both pins must be grounded.
7	BOOT	Internal MOSFET gate driver bootstrap. Connect a 0.1 μ F X7R ceramic capacitor from this pin to LX pin.
8	LX	Internal high-side MOSFET switch output. Connect this pin to the inductor and Schottky diode.
	Thermal Pad	Connect to GND.

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ORDERING INFORMATION

Automotive Range: -40°C to +125°C

Order Part No.	Package	QTY/Reel
IS32LT3953B-GRLA3-TR	SOP-8-EP, Lead-free	2500

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- a.) the risk of injury or damage has been minimized;
- b.) the user assume all such risks; and
- c.) potential liability of Lumissil Microsystems is adequately protected under the circumstances

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ABSOLUTE MAXIMUM RATINGS (Note 1)

Input voltage, V_{CC} (Note 2)	-0.3V ~ +42V
Bootstrap to switching voltage, ($V_{BOOT} - V_{LX}$)	-0.3V ~ +6.0V
Switching voltage, V_{LX} (Steady state)	-0.6V ~ $V_{CC} + 0.3V$
Switching voltage, V_{LX} (Transient < 10ns)	-3.0V
EN/PWM and TON voltage, $V_{EN/PWM}$ and V_{TON}	-0.3V ~ $V_{CC} + 0.3V$
VDD and FB voltage, V_{DD} and V_{FB}	-0.3V ~ 6.0V
Power dissipation, $P_{D(MAX)}$	2.34W
Operating temperature, $T_A = T_J$	-40°C ~ +150°C
Storage temperature, T_{STG}	-65°C ~ +150°C
Junction temperature, T_{JMAX}	+150°C
Junction Package thermal resistance, junction to ambient (4 layer standard test PCB based on JESD 51-2A), θ_{JA}	42.7°C/W
Package thermal resistance, junction to thermal PAD (4 layer standard test PCB based on JESD 51-8), θ_{JP}	1.41°C/W
ESD (HBM)	±2kV
ESD (CDM)	±750V

Note 1: Stresses beyond those listed under "Absolute Maximum Ratings" may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other condition beyond those indicated in the operational sections of the specifications is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

Note 2: A maximum of 44V can be sustained at this pin for a duration of ≤ 2s.

ELECTRICAL CHARACTERISTICS

$V_{CC} = 24V$, $T_J = T_A = -40^\circ C \sim +125^\circ C$, Typical values are at $T_J = 25^\circ C$, unless otherwise noted.

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
V_{CC}	Input supply voltage		4.5		38	V
V_{UVLO}	VCC undervoltage lockout threshold	V_{CC} increasing	4.05	4.25	4.45	V
V_{UVLO_HY}	VCC undervoltage lockout hysteresis	V_{CC} decreasing		250		mV
I_{CC}	VCC pin supply current	$V_{FB} = 0.5V$, $V_{EN/PWM} = \text{high}$		1.2	2	mA
I_{SD}	VCC pin shutdown current	EN/PWM shorted to GND		2	10	μA
V_{DD}	Regulator output voltage	$I_{DD} < 5mA$, $V_{CC} > 6V$	5.0	5.2	5.4	V
I_{DD_LIM}	Regulator output current limit	$V_{CC} = 12V$, $V_{DD} = 0V$	20	40		mA
I_{SWLIM}	Buck switch current limit threshold		3.5	4.5	5.5	A
t_{OCP}	Over Current Protection (OCP) hiccup time	(Note 3)		1		ms
R_{DS_ON}	Buck switch on-resistance	$V_{BOOT} = V_{CC} + 4.3V$, $I_{LX} = 1A$		0.2	0.4	Ω
V_{BTUV}	BOOT undervoltage lockout threshold	V_{BOOT} to V_{LX} increasing		3.3		V
V_{BTUV_HY}	BOOT undervoltage lockout hysteresis	V_{BOOT} to V_{LX} decreasing		400		mV
t_{OFF_MIN}	Switching minimum off-time	$V_{FB} = 0V$		110	150	ns
t_{ON_MIN}	Switching minimum on-time			120	150	ns
t_{ON}	Selected on-time	$V_{CC} = 24V$, $V_{OUT} = 12V$, $R_{TON} = 420k\Omega$	800	1000	1200	ns
Regulation Comparator and Error Amplifier						
V_{FB}	Load current sense regulation threshold	V_{FB} decreasing, LX turns on, $T_J = 25^\circ C$	195	200	205	mV
		V_{FB} decreasing, LX turns on, $T_J = -40^\circ C \sim 125^\circ C$	190	200	210	

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ELECTRICAL CHARACTERISTICS (CONTINUE)

$V_{CC} = 24V$, $T_A = T_J = -40^{\circ}C \sim +125^{\circ}C$, Typical values are at $T_J = 25^{\circ}C$, unless otherwise noted.

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
Enable Input						
V_{IH}	Logic high voltage	$V_{EN/PWM}$ increasing	1.4			V
V_{IL}	Logic low voltage	$V_{EN/PWM}$ decreasing			0.4	V
R_{PWMPD}	EN/PWM pin pull-down resistance	$V_{EN/PWM} = 5V$	100	200	300	k Ω
t_{PWML}	Duration EN/PWM pin kept low to shutdown the device		105	130	155	ms
t_{PWMH}	Duration EN/PWM pin kept high to quit from shutdown mode	(Note 3)		16	30	μs
t_{PWMSW}	The latency of EN/PWM pull high to IC starts switching	(Note 3)		120	150	μs
Thermal Shutdown						
T_{SD}	Thermal shutdown threshold	(Note 3)		165		$^{\circ}C$
T_{SDHYS}	Thermal shutdown hysteresis	(Note 3)		25		$^{\circ}C$

Note 3: Guaranteed by design.

TYPICAL PERFORMANCE CHARACTERISTICS

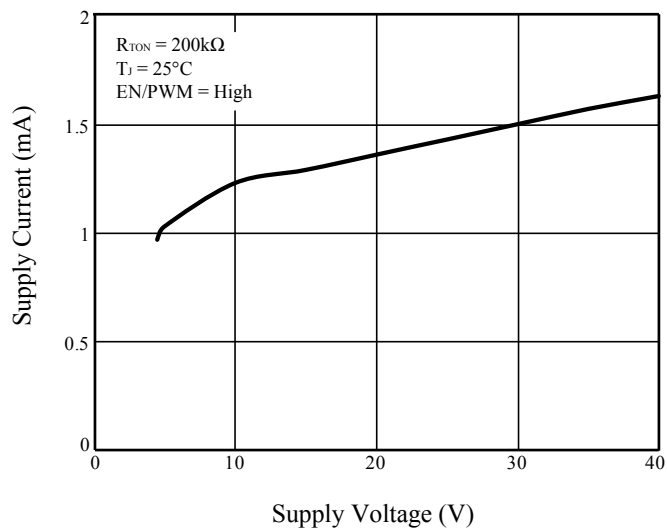


Figure 4 I_{CC} vs. V_{CC}

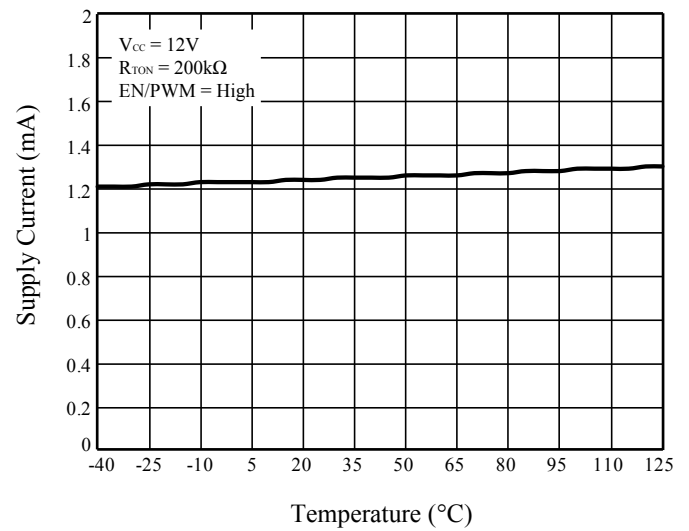


Figure 5 I_{CC} vs. Temperature

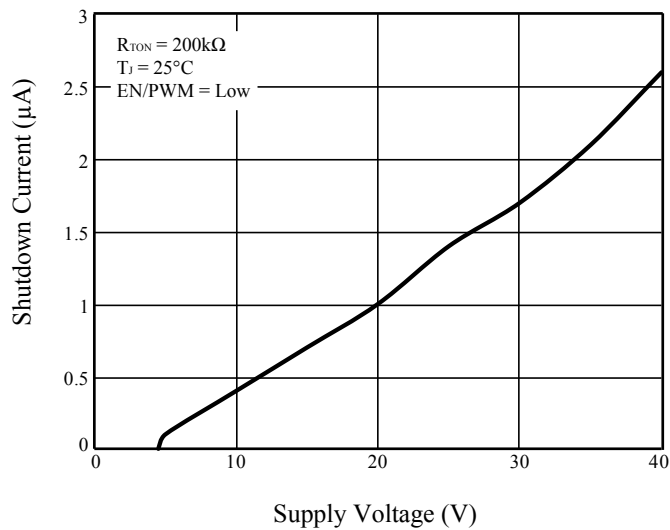


Figure 6 I_{SD} vs. V_{CC}

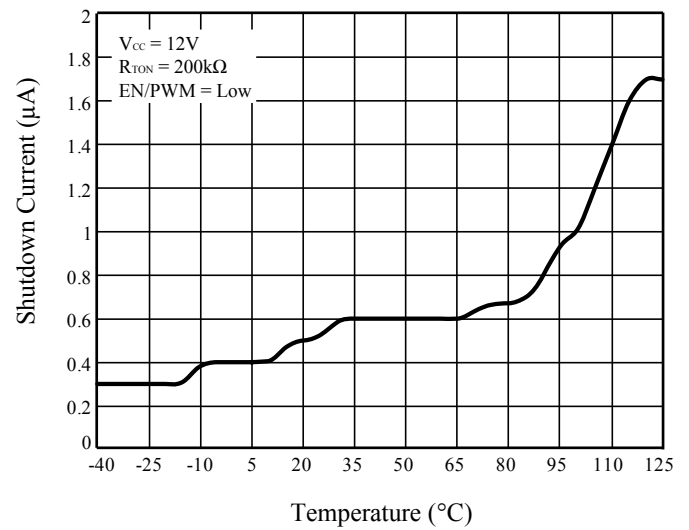


Figure 7 I_{SD} vs. Temperature

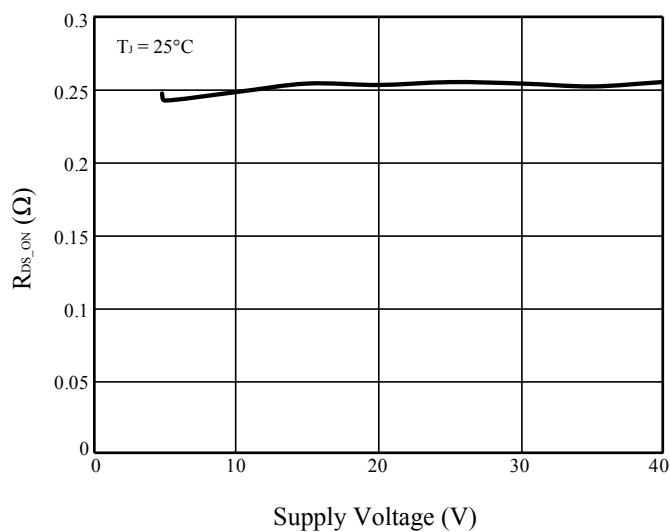


Figure 8 R_{DS_ON} vs. V_{CC}

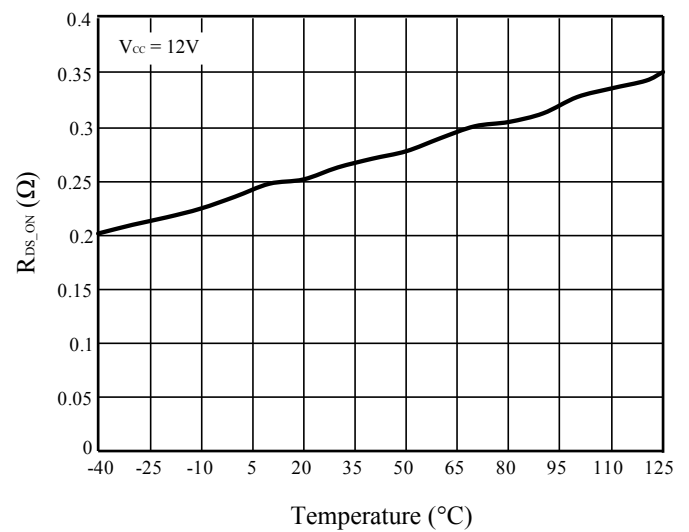


Figure 9 R_{DS_ON} vs. Temperature

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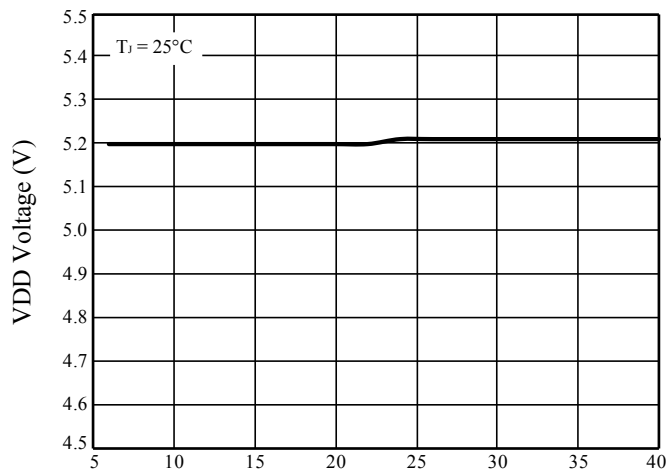


Figure 10 V_{DD} vs. V_{CC}

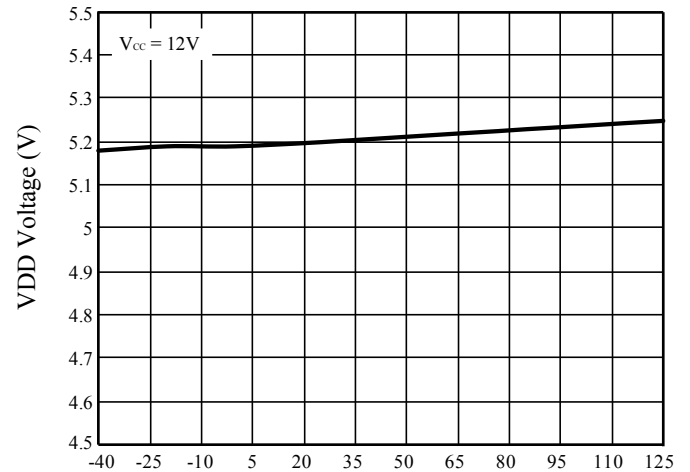


Figure 11 V_{DD} vs. Temperature

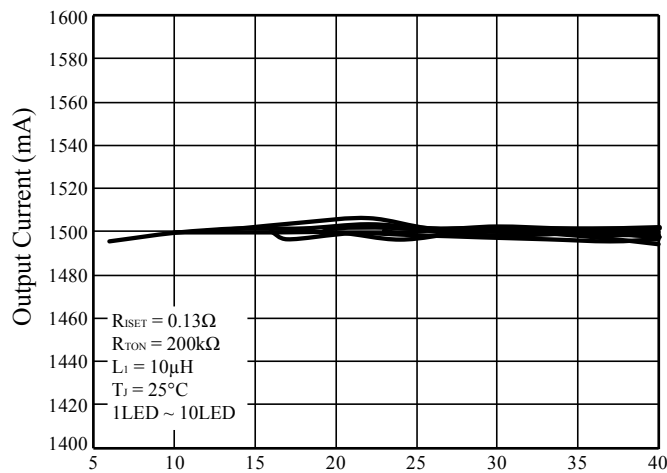


Figure 12 I_{OUT} vs. V_{CC}

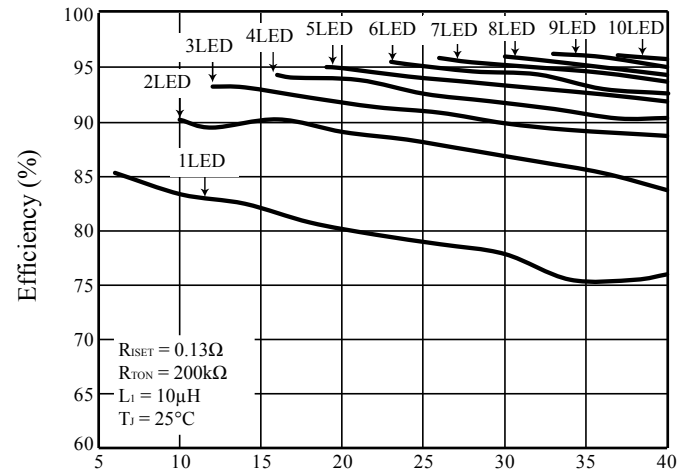


Figure 13 Efficiency vs. V_{CC}

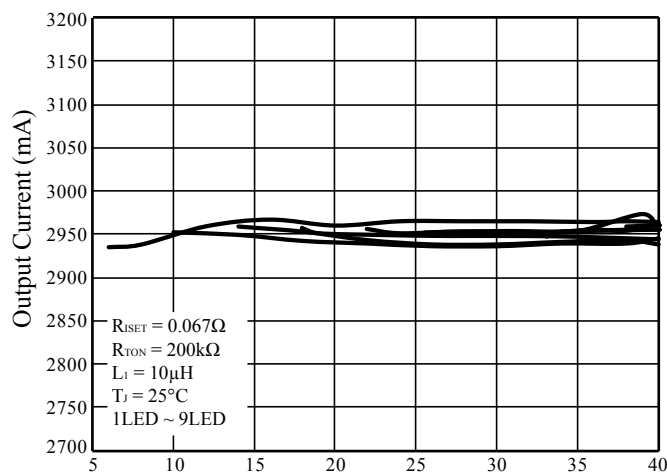


Figure 14 I_{OUT} vs. V_{CC}

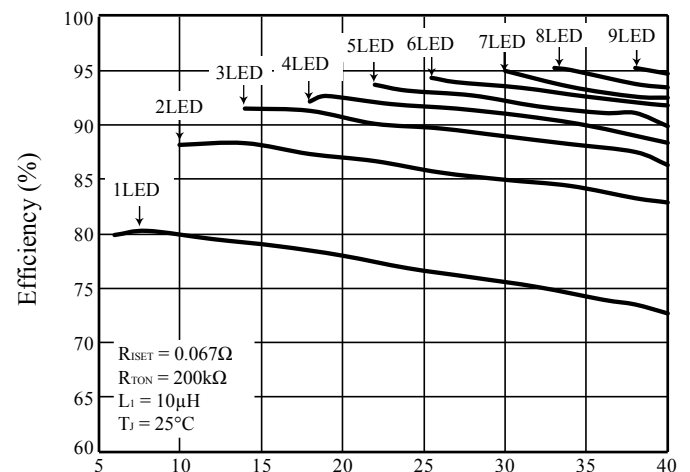


Figure 15 Efficiency vs. V_{CC}

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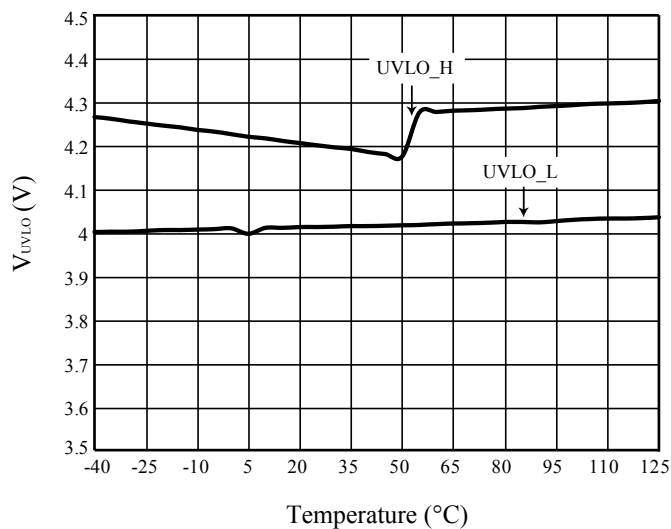


Figure 16 V_{UVLO} vs. Temperature

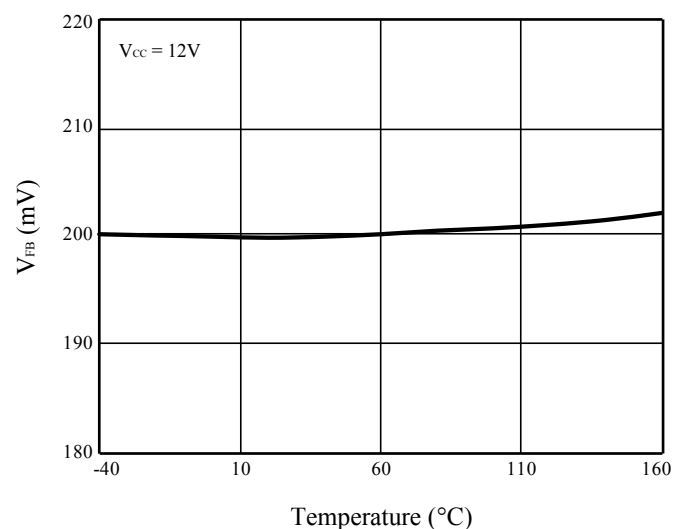


Figure 17 V_{FB} vs. Temperature

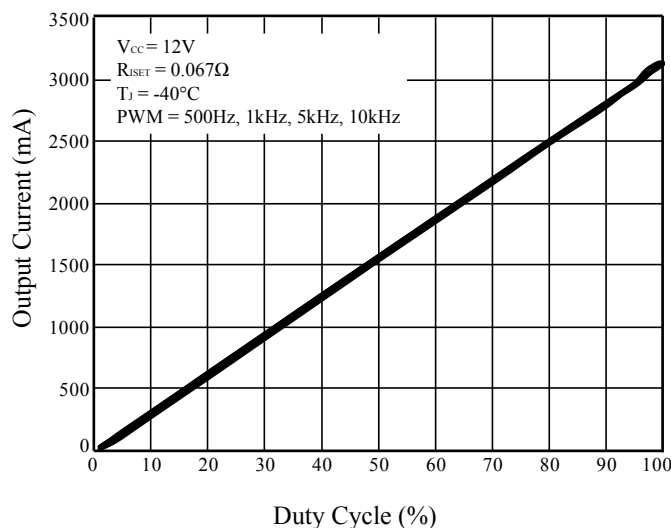


Figure 18 I_{OUT} vs. Duty Cycle

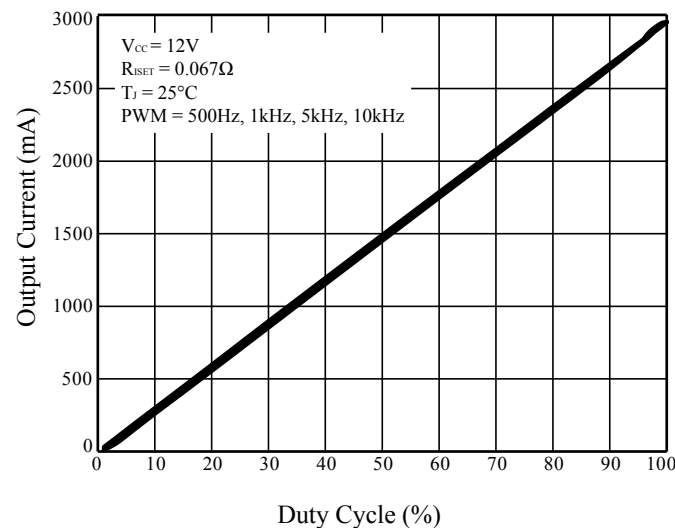


Figure 19 I_{OUT} vs. Duty Cycle

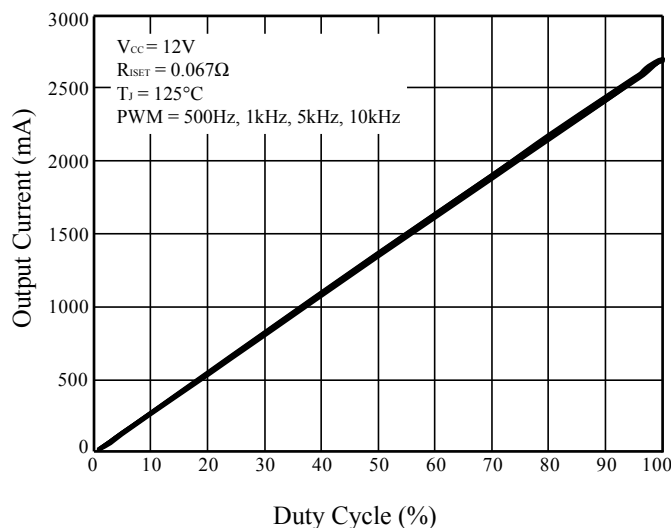


Figure 20 I_{OUT} vs. Duty Cycle

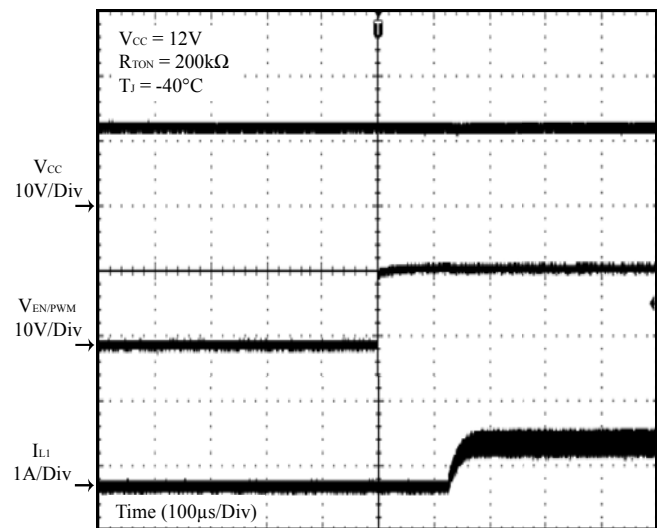


Figure 21 EN/PWM Enable Time

IS32LT3953B

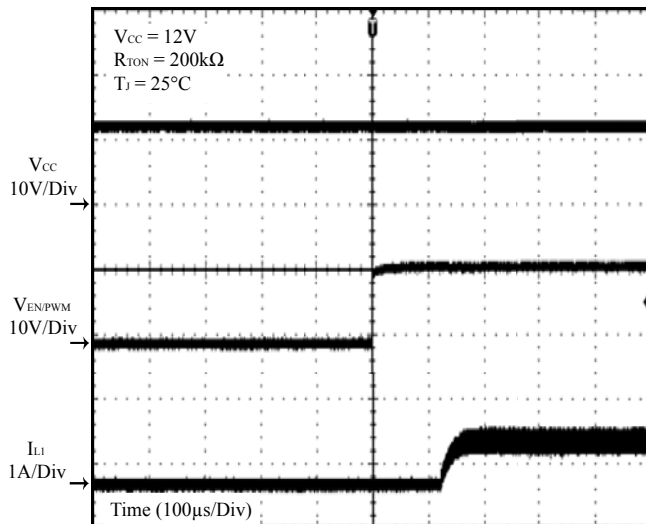


Figure 22 EN/PWM Enable Time

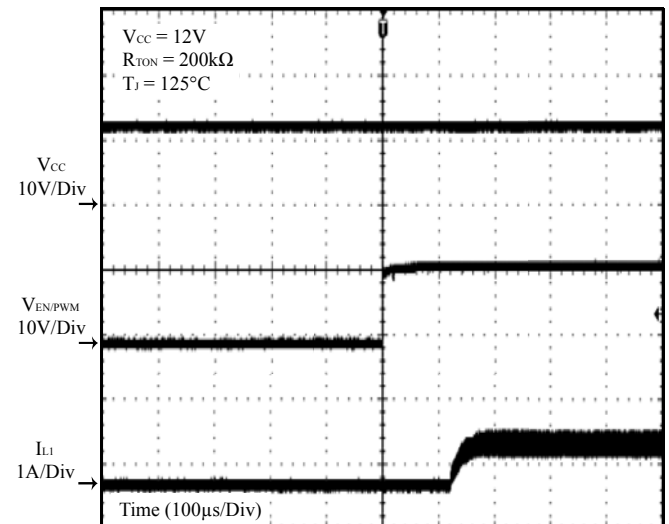


Figure 23 EN/PWM Enable Time

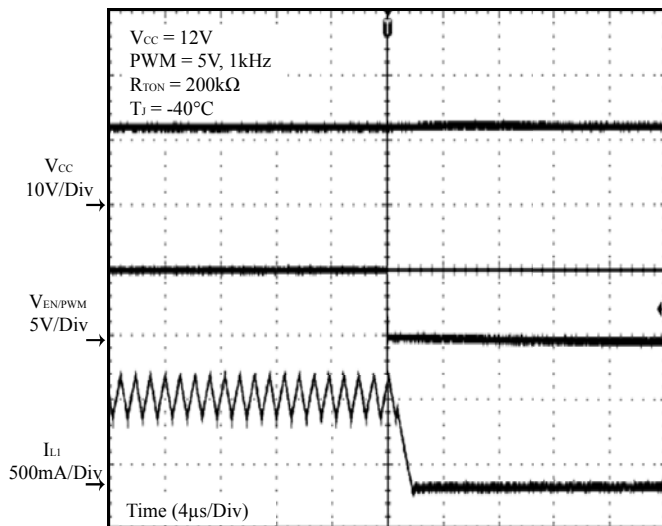


Figure 24 PWM Off

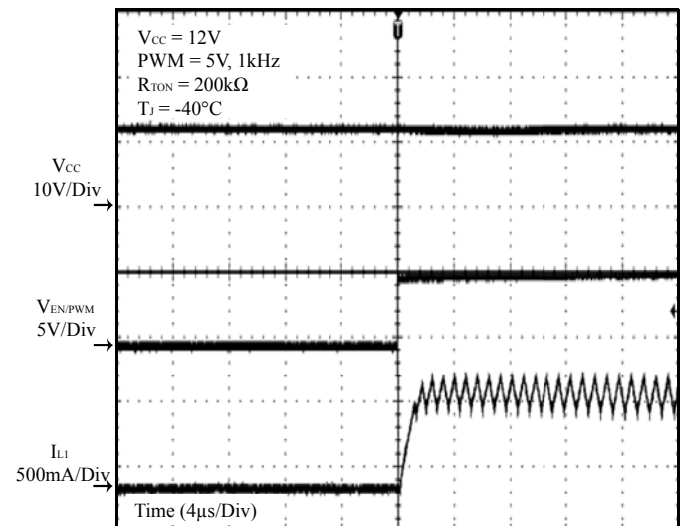


Figure 25 PWM On

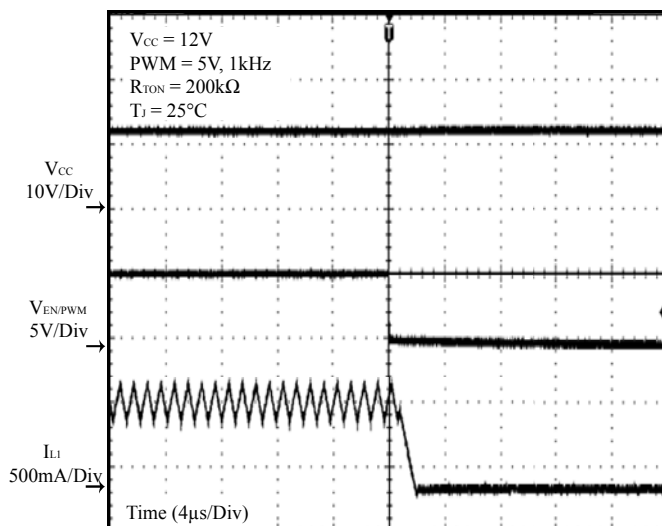


Figure 26 PWM Off

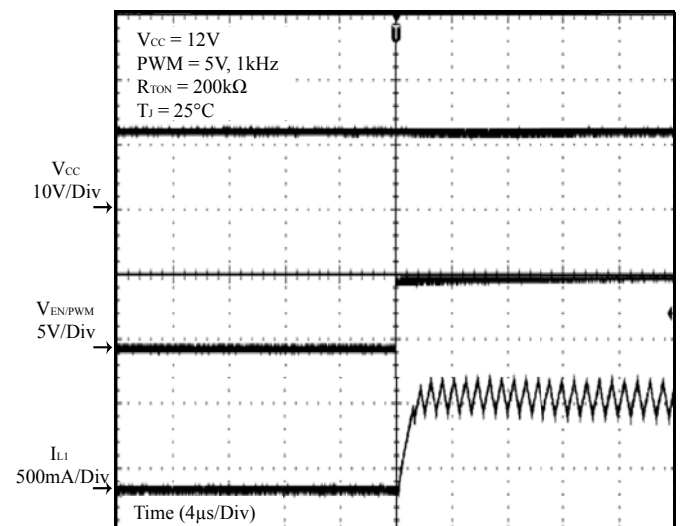


Figure 27 PWM On

IS32LT3953B

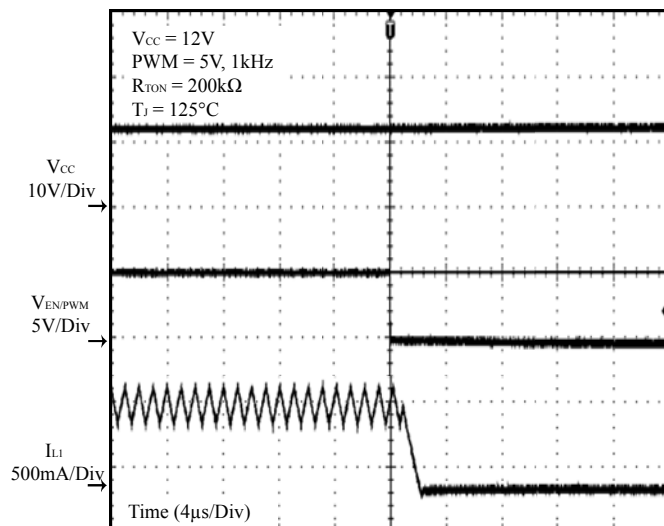


Figure 28 PWM Off

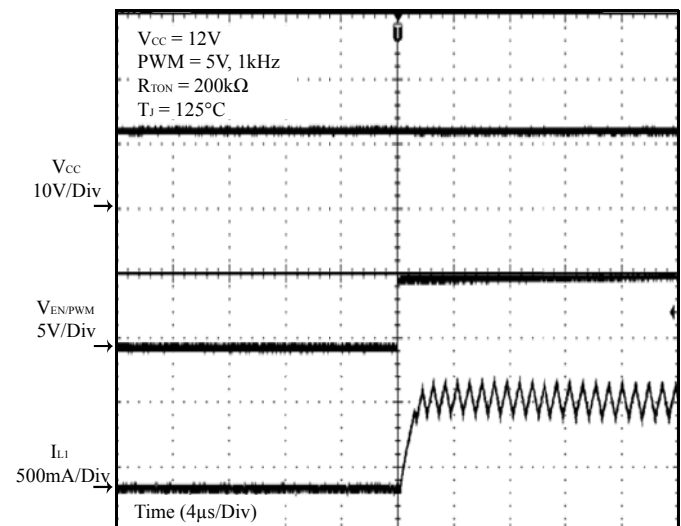
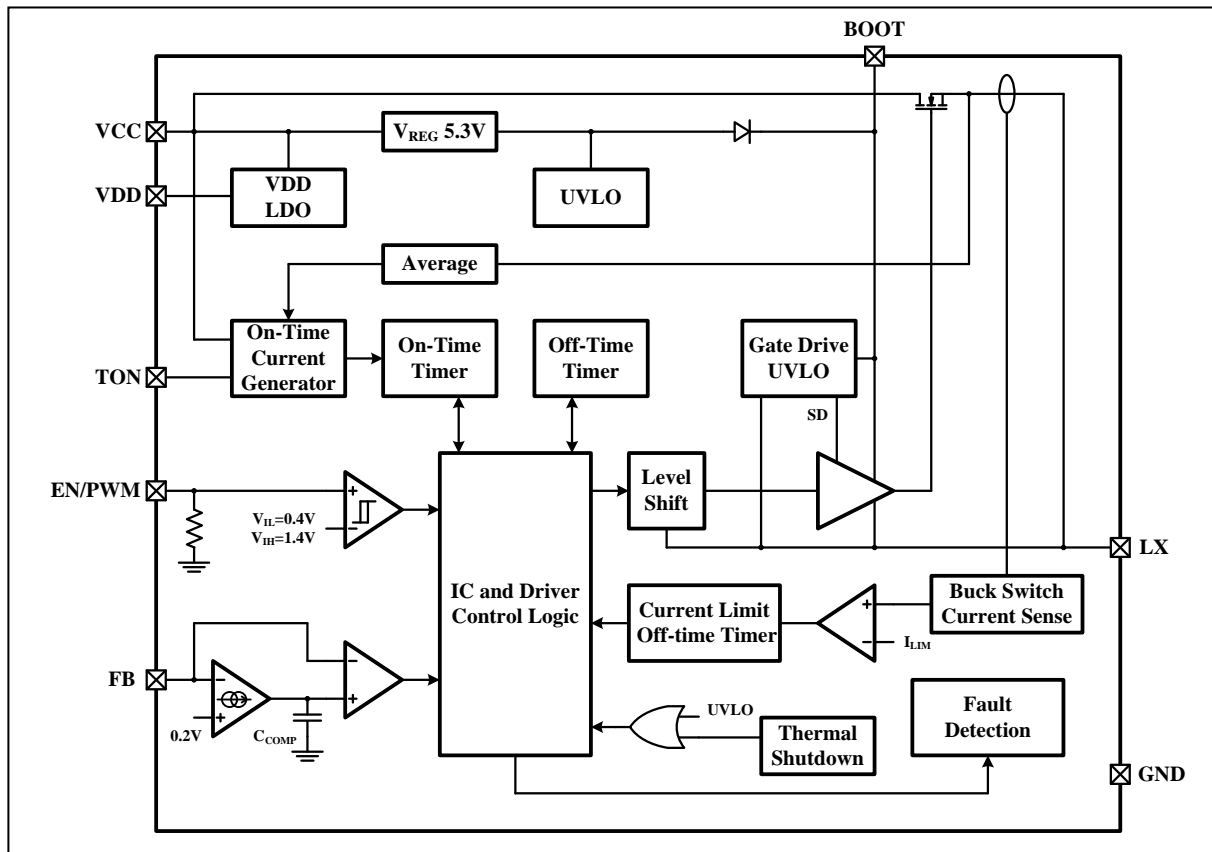


Figure 29 PWM On

FUNCTIONAL BLOCK DIAGRAM



IS32LT3953B

APPLICATION INFORMATION

DESCRIPTION

The IS32LT3953B is a buck regulator with wide input voltage, low reference voltage, quick output response and excellent PWM dimming performance, which is ideal for driving a high-current LED string. It uses average current mode control to maintain constant LED current and consistent brightness.

UNDER VOLTAGE LOCKOUT (UVLO)

The device features an under voltage lockout (UVLO) function on VCC pin. This is a fixed value which cannot be adjusted. The device is enabled when the VCC voltage rises to exceed V_{UVLO} (Typ. 4.25V), and disabled when the VCC voltage falls below ($V_{UVLO} - V_{UVLO_HY}$) (Typ. 4.0V).

LINEAR REGULATOR VDD

The device incorporates a linear regulator (VDD) to supply current for the device operation as well as additional power for external circuitry. It requires a low ESR, X7R type ceramic capacitor from VDD pin to GND for proper operation; this capacitor must be placed as close to VDD pin as possible. The recommended capacitor value is 0.47 μ F.

BOOTSTRAP CIRCUIT

The gate driver of the integrated high-side MOSFET requires a voltage above VCC. As below circuit diagram, there is a dedicated 5.3V LDO which is the power supply of the gate driver. The BOOT pin is internally connected to the output of the 5.3V LDO. Connect a ceramic capacitor between BOOT and SW pins. The VCC supplies the power to the 5.3V LDO which charges the C_{BOOT} capacitor during high-side MOSFET off cycles. Then in high-side MOSFET on cycles, the C_{BOOT} charge voltage is used to boost the BOOT pin to 5.3V higher than LX pin.

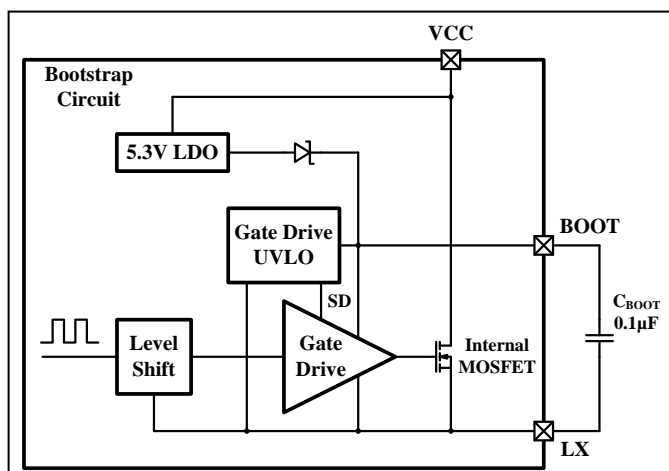


Figure 30 Bootstrap Circuit

A 0.1 μ F X7R ceramic capacitor will work well in most applications. The gate driver also has an under voltage lockout detection. The gate driver is enabled when the

voltage on the C_{BOOT} rises above V_{BTUV} (Typ. 3.3V), and disabled when the voltage on the C_{BOOT} drops below ($V_{BTUV} - V_{BTUV_HY}$) (Typ. 2.9V).

OUTPUT CURRENT SETTING

The LED current is configured by an external sense resistor, R_{ISET} , with a value determined as follows Equation (1):

$$I_{LED} = V_{FB} / R_{ISET} \quad (1)$$

Where $V_{FB} = 0.2V$ (Typ.).

Note that $R_{ISET} = 0.0667\Omega$ is the minimum allowed value for the sense resistor in order to maintain the switch current below the specified maximum value.

Table 1 R_{ISET} Resistance Versus Output Current

$R_{ISET} (\Omega)$	Nominal Average Output Current (mA)
0.2	1000
0.1	2000
0.0667	3000

The resistor R_{ISET} should be a 1% resistor with enough power tolerance and good temperature characteristic to ensure accurate and stable output current.

ENABLE AND PWM DIMMING

A high logic signal on the EN/PWM pin will enable the IC. The buck converter ramps up the LED current to a target level which is set by external resistor, R_{ISET} .

When the EN/PWM pin goes from high to low, the buck converter will turn off, but the IC remains in standby mode for up to t_{PWML} . When the EN/PWM pin goes high within this period, the LED current will turn on immediately. Sending a PWM (pulse-width modulation) signal to the EN/PWM pin will result in dimming of the LED. The resulting LED brightness is proportional to the duty cycle (t_{ON} / T) of the PWM signal. A practical range for PWM dimming frequency is between 100Hz and 20kHz.

There is an inherent PWM turn on delay time of about 1 μ s during continuous PWM dimming. A high frequency PWM signal has a shorter period time that will degrade the PWM dimming linearity. Therefore, a low frequency PWM signal is good for achieving better dimming contrast ratio. At a 200Hz PWM frequency, the dimming duty cycle can be varied from 100% down to 1% or lower.

If the EN/PWM pin is kept low for at least t_{PWML} , the IC enters shutdown mode to reduce power consumption. The next high signal on EN/PWM will initialize a full startup sequence, which includes a shutdown quit time, t_{PWMLH} , and a startup latency, t_{PWMSW} . This startup sequence does not exist in a typical PWM operation.

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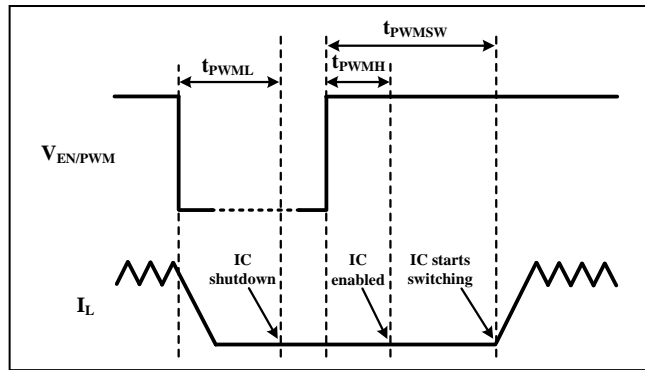


Figure 31 Device Shutdown and Enable

The EN/PWM pin is high-voltage tolerant and can be connected directly to a power supply. However, a series resistor (10kΩ) is required to limit the current flowing into the EN pin if PWM is higher than the V_{CC} voltage at any time. If PWM is driven from a logic input, this series resistor is not necessary.

ANALOG DIMMING

To realize analog dimming, it needs to offset an external DC voltage to FB pin by two pieces of low cost resistors. As Figure 32 typical schematic of analog dimming, R_{DIM1} and R_{DIM2} resistor network is added on FB pin. In close loop operating, the FB pin will be regulated by the device to maintain its voltage at the threshold, typical 200mV. So in below calculation, the V_{FB} is a known value, 0.2V.

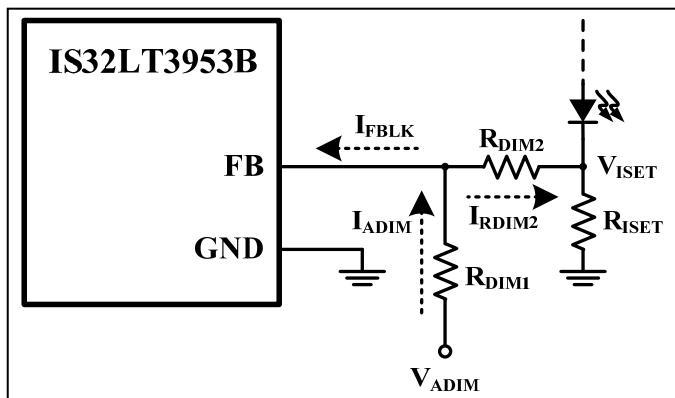


Figure 32 Adding Output Capacitor

When an external DC voltage V_{ADIM} apply to R_{DIM1}, the current I_{ADIM} is generated, which can be calculated by:

$$I_{ADIM} = \frac{V_{ADIM} - V_{FB}}{R_{DIM1}} \quad (2)$$

The current in R_{DIM2} is:

$$I_{RDIM2} = I_{ADIM} - I_{FBLK} \quad (3)$$

Where, I_{FBLK} is the leakage current of FB pin. Since the FB pin is high impedance pin whose leakage current is enough tiny to be neglected. So the R_{DIM1}'s current is almost equal to R_{DIM2}'s current:

$$I_{RDIM2} \approx I_{ADIM} = \frac{V_{ADIM} - V_{FB}}{R_{DIM1}} \quad (4)$$

Then R_{ISET} resistor voltage is:

$$V_{ISET} = V_{FB} - \frac{V_{ADIM} - V_{FB}}{R_{DIM1}} \times R_{DIM2} \quad (5)$$

And the actual LED output current is:

$$I_{LED} = (V_{FB} - \frac{V_{ADIM} - V_{FB}}{R_{DIM1}} \times R_{DIM2}) / R_{ISET} \quad (6)$$

According to above Equation (5), when R_{DIM1}, R_{DIM2} and R_{ISET} are selected, the LED current I_{LED} can be adjusted by V_{ADIM} voltage. And I_{LED} is reversely proportional to V_{ADIM}, the higher V_{ADIM} the lower LED current. When V_{ADIM} is 0.2V, the V_{ISET} is equal to V_{FB}. As Figure 33 graph. The recommended R_{DIM2} value is 1kΩ.

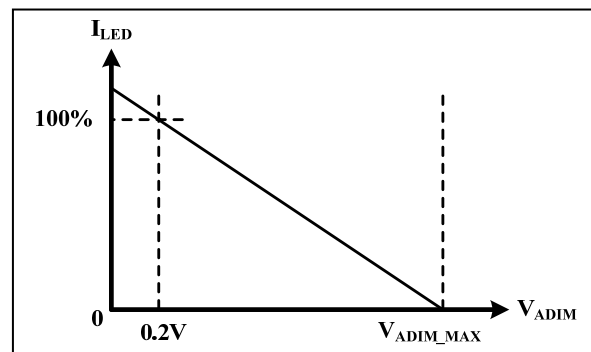


Figure 33 Analog Dimming Voltage vs LED Current

For analog dimming, the current error at low level due to the leakage current of FB pin (I_{FBLK}) could be significant. So the recommended lowest percentage level of analog dimming is 5%. To achieve high accurate dimming at low level, the PWM dimming is better solution.

INPUT CAPACITOR

The input capacitor provides the transient pulse current, which is approximately equal to I_{LED}, to the inductor of the converter when the high-side MOSFET is on. An X7R type ceramic capacitor is a good choice for the input bypass capacitor to handle the ripple current since it has a very low equivalent series resistance (ESR) and low equivalent series inductance (ESL). Use the following equation to estimate the approximate capacitance:

$$C_{IN_MIN} = \frac{I_{LED} \times t_{ON}}{\Delta V_{CC}} \quad (7)$$

Where, ΔV_{CC} is the acceptable input voltage ripple, generally choose 5%-10% of input voltage. t_{ON} is on-time of the high-side MOSFET in μs. A minimum input capacitance of 2X C_{IN_MIN} is recommended for most applications.

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OUTPUT CAPACITOR

The IS32LT3953B control loop can accept a voltage ripple on the FB pin, this means it can operate without an output capacitor to save cost. The FB pin needs a certain amount of voltage ripple to keep control loop stability. A capacitor can be added across the LEDs but excluding the FB resistor. This capacitor will reduce the LED current ripple while keep the same average current in some application cases. The reduction of the LED current ripple by the capacitor depends on several factors: capacitor value, inductor current ripple, operating frequency, output voltage, etc. A several μF capacitor is sufficient for most applications. However, the output capacitor brings in more delay time of LED current during PWM dimming that will degrade the dimming contrast.

The output capacitor is used to filter the LED current ripple to an acceptable level. The equivalent series resistance (ESR), equivalent series inductance (ESL) and capacitance of the capacitor contribute to the output current ripple. Therefore, a low-ESR X7R type capacitor should be used.

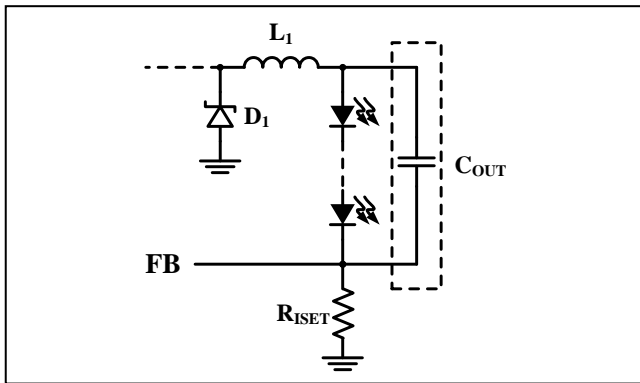


Figure 34 Adding Output Capacitor

FREQUENCY SELECTION

During switching the IS32LT3953B operates in a constant on-time mode. The on-time is adjusted by the external resistor, R_{TON} , which is connected between the VCC and TON pins.

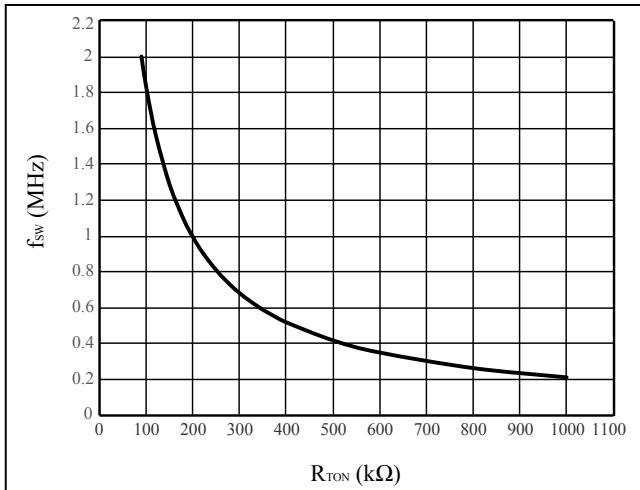


Figure 35 Operating Frequency vs. R_{TON} Resistance

The approximate operating frequency can be calculated by below Equation (8) and (9):

$$t_{ON} = \frac{k \times (R_{TON} + R_{INT}) \times V_{OUT}}{V_{CC}} \quad (8)$$

$$f_{sw} = \frac{1}{k \times (R_{TON} + R_{INT})} \quad (9)$$

Where $k = 0.00458$, with f_{sw} in MHz, t_{ON} in μs , and R_{TON} and R_{INT} (internal resistance, 20k Ω) in k Ω .

Higher frequency operation results in smaller component size but increases the switching losses. It may also increase the high-side MOSFET gate driving current and may not allow sufficient high or low duty cycle. Lower frequency gives better performance but results in larger component size.

SPREAD SPECTRUM

A switch mode controller can be troublesome when the EMI is concerned. To optimize the EMI performance, the IS32LT3953B includes a spread spectrum feature, which is a 500Hz with $\pm 10\%$ operating frequency jitter. The spread spectrum can spread the total electromagnetic emitting energy into a wider range that significantly degrades the peak energy of EMI. With spread spectrum, the EMI test can be passed with smaller size and lower cost filter circuit.

MINIMUM AND MAXIMUM OUTPUT VOLTAGE

The output voltage of a buck converter is approximately given as below:

$$V_{OUT} = V_{CC} \times D \quad (10)$$

Where D is the operating duty cycle.

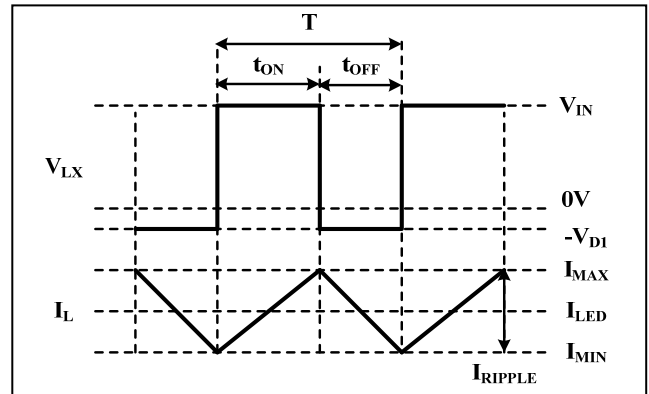


Figure 36 Operating Waveform

$$D = \frac{t_{ON}}{t_{ON} + t_{OFF}} \quad (11)$$

$$\text{So, } V_{OUT} = V_{CC} \times \frac{t_{ON}}{t_{ON} + t_{OFF}} = V_{CC} \times t_{ON} \times f_{sw} \quad (12)$$

Where t_{ON} and t_{OFF} are the turn-on and turn off time of

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high-side MOSFET. Note that due to the spread spectrum, the f_{SW} should use the maximum of the operating frequency, $110\% \times f_{SW}$.

According to above equation, the output voltage depends on the operating frequency and the high-side MOSFET turn on time. When the frequency is set, the maximum output voltage is limited by the switching minimum off-time t_{OFF_MIN} , about 150ns. For example, if the input voltage is 12V and the operating frequency $f_{SW}=1\text{MHz}$, the maximum output voltage is:

$$V_{OUT} = 12V \times (1\mu s - 150ns) \times 1MHz = 10.2V \quad (13)$$

Assume the forward voltage of each LED is 3.2V, the device can drive up to 3 LEDs in series.

The minimum output voltage is limited by the switching minimum on-time, about 150ns, since the frequency is set. For example, if the input voltage is 12V and the operating frequency $f_{SW}=1\text{MHz}$, the minimum output voltage is:

$$V_{OUT} = 12V \times 150ns \times 1MHz = 1.8V \quad (14)$$

This means the device can drive a low forward voltage LED, such as a RED color LED. So under the condition of $V_{CC}=12V$ and $f_{SW}=1\text{MHz}$, the output voltage range is 1.8V~10.2V. Exceeding this range, the operation will be clamped and the output current cannot reach the set value.

In a typical application, the output voltage is affected by other operating parameters, such as output current, R_{DS_ON} of the high-side MOSFET, DRC of the inductor, parasitic resistance of the PCB traces, and the forward voltage of the diode. Therefore, the output voltage range could vary from the calculation. The more precision equation is given by:

$$V_{OUT} = (V_{CC} - I_{LED} \times R_{DS_ON}) \times D - R_L \times I_{LED} - V_D \times (1 - D) \quad (15)$$

Where, R_{DS_ON} is the static drain-source on resistance of the high-side MOSFET, and R_L is the inductor DC resistance.

Figure 37 shows how the minimum and maximum output voltages vary with the operating frequency at 12V and 24V input. Figure 38 shows how the minimum and maximum output voltages vary with the LED current at 9V input (assuming $R_{DS_ON} = 0.4\Omega$, inductor DCR $R_L = 0.1\Omega$, and diode $V_D = 0.6V$). Note that due to spread spectrum the f_{SW} should use the maximum operating frequency, $110\% \times f_{SW}$.

When the output voltage is lower than the minimum t_{ON} time of the device, the device will automatically extend the operating t_{OFF} time to maintain the set output LED current all the time. However, the operating frequency will decrease accordingly to lower level to keep the duty cycle in correct regulating.

To achieve wider output voltage range and flexible output configuration, a lower operating frequency

could be considered.

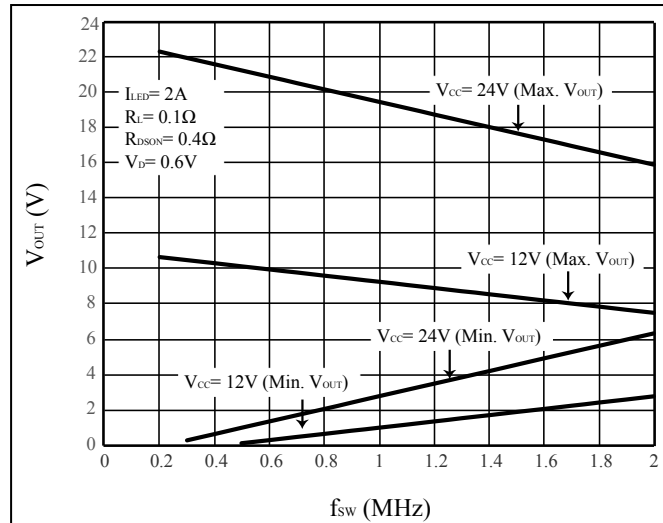


Figure 37 Minimum and Maximum Output Voltage versus Operating Frequency (minimum t_{ON} and $t_{OFF} = 150ns$)

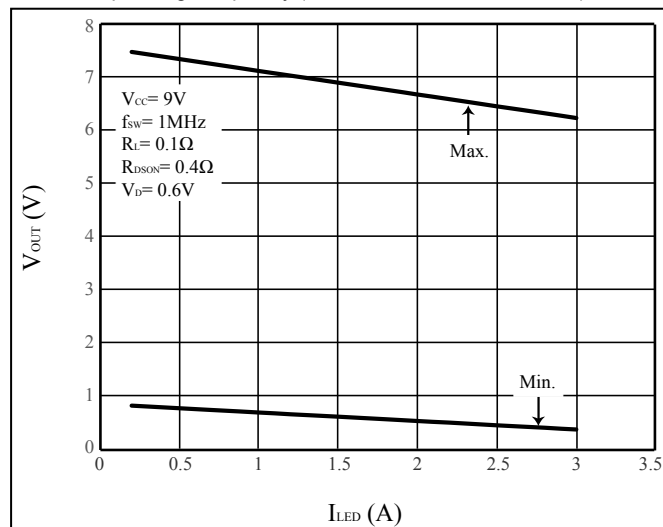


Figure 38 Minimum and Maximum Output Voltage versus LED Current (minimum t_{ON} and $t_{OFF} = 150ns$)

PEAK CURRENT LIMIT

To protect itself, the IS32LT3953B integrates an Over Current Protection (OCP) detection circuit to monitor the current through the high-side MOSFET during switching on. Whenever the current exceeds the OCP current threshold, I_{SW_LIM} , the device will immediately turn off the high-side MOSFET for t_{OCP} and restart again. The device will remain in this hiccup mode until the current drops below I_{SW_LIM} .

INDUCTOR

Inductor value involves trade-offs in performance. A larger inductance reduces output current ripple, however it also brings in unwanted parasitic resistance that degrades the efficiency. A smaller inductance has compact size and lower cost, but introduces higher ripple in the LED string. Use the following equation to estimate the approximate inductor value:

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$$L = \frac{(V_{CC} - V_{LED}) \times V_{LED}}{f_{SW} \times \Delta I_L \times V_{CC}} \quad (16)$$

Where V_{CC} is the minimum input voltage in volts, V_{LED} is the total forward voltage of LED string in volts, f_{SW} is the operation frequency in hertz and ΔI_L is the current ripple in the inductor. Select an inductor with a rated current greater than the output average current and the saturation current over the Over Current Protection (OCP) current threshold I_{SWLIM} .

Since the IS32LT3953B is a Continuous Conduction Mode (CCM) buck driver which means the valley of the inductor current, I_{MIN} , should not drop to zero at any time, the ΔI_L must be smaller than 200% of the average output current.

$$I_{MIN} = I_{LED} - \frac{\Delta I_L}{2} > 0 \quad (17)$$

Besides, the peak current of the inductor, I_{MAX} , must be smaller than I_{SWLIM} to prevent the IS32LT3953B from triggering OCP, especially when the output current is set to a high level.

$$I_{MAX} = I_{LED} + \frac{\Delta I_L}{2} < I_{SWLIM} \quad (18)$$

To ensure system stability, the ΔI_L must be higher than 10% of the average output current. For better performance, choose an inductor current ripple ΔI_L between 10% and 50% of the average output current.

$$0.1 \times I_{LED} \leq \Delta I_L \leq 0.5 \times I_{LED} \quad (19)$$

Figure 39 shows inductor selection based on the operating frequency and LED current at 30% inductor current ripple. If a lower operating frequency is used, either a larger inductance or current ripple should be used.

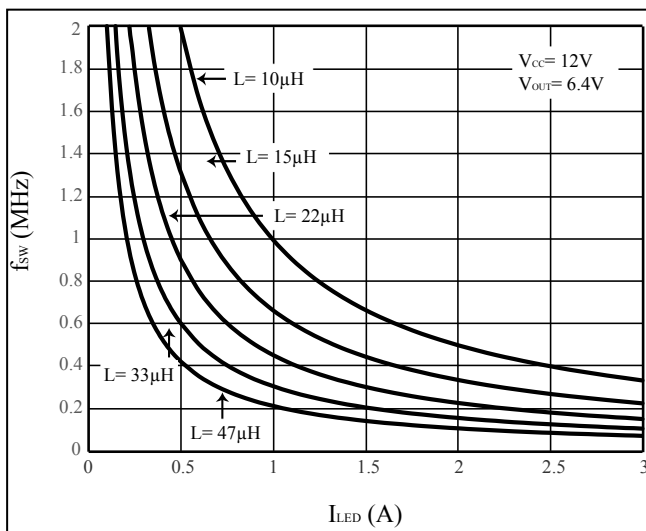


Figure 39 Inductance Selection Based On 30% Current Ripple

DIODE

The IS32LT3953B is a non-synchronous buck driver that requires a recirculating diode to conduct the current during the high-side MOSFET off time. The best choice is a Schottky diode due to its low forward voltage, low reverse leakage current and fast reverse recovery time. The diode should be selected with a peak current rating above the inductor peak current and a continuous current rating higher than the maximum output load current. It is very important to consider the reverse leakage of the diode when operating at high temperature. Excess leakage will increase the power dissipation on the device.

The higher input voltage and the voltage ringing due to the reverse recovery time of the Schottky diode will increase the peak voltage on the LX output. If a Schottky diode is chosen, care should be taken to ensure that the total voltage appearing on the LX pin including supply ripple, does not exceed its specified maximum value.

THERMAL SHUTDOWN PROTECTION

To protect the IC from damage due to high power dissipation, the temperature of the die is monitored. If the die temperature exceeds the thermal shutdown temperature of 165°C (Typ.) then the device will shut down, and the output current is shut off. After a thermal shutdown event, the IS32LT3953B will not try to restart until its temperature has reduced to less than 140°C (Typ.).

FAULT HANDLING

The IS32LT3953B is designed to detect the following faults:

- Pin open
- Pin-to-ground short (except LX pin)
- Pin-to-neighboring pin short
- Output LED string open and short
- External component open or short (except diode)
- Thermal shutdown

Please check Table 2 for the details of the fault actions.

Table 2 Fault Actions

Fault Type	LED String	Detect Condition	Fault Recovering
Inductor shorted	Dim	Trigger OCP. Turn off high-side MOSFET immediately. Retry after 1ms.	Inductor shorted removed. No OCP triggered.
R _{ISET} short	Dim	Trigger OCP. Turn off high-side MOSFET immediately. Retry after 1ms.	R _{ISET} shorted removed. No OCP triggered.
R _{ISET} open	Off	The FB pin voltage exceeds 2V. Turn off high-side MOSFET immediately. Retry after 1ms.	R _{ISET} open removed. The FB pin voltage drops below 1.55V.
LED string shorted to GND	Off	Trigger OCP. Turn off high-side MOSFET immediately. Retry after 1ms.	Shorted removed. No OCP triggered.
BOOT capacitor open	Dim	V _{CC} -V _{sw} >1.8V at high-side MOSFET ON (High-side can't fully turn on). Turn off high-side MOSFET immediately. Retry after 1ms.	BOOT capacitor open removed
BOOT capacitor shorted	Off	Bootstrap circuit UVLO and turn off high-side MOSFET immediately.	BOOT capacitor shorted removed. Release from UVLO.
R _{TON} resistor open	Dim	On-time exceeds 20μs or trigger OCP, then turn off high-side MOSFET immediately. Retry after 1ms.	R _{TON} resistor open removed. No over 20μs on-time or OCP triggered.
R _{TON} resistor shorted	Dim	The device operating at minimum on/off time, maybe trigger the other fault conditions.	R _{TON} resistor shorted removed.
EN short to R _{ISET}	Off	EN/PWM will be pulled low by R _{ISET} resistor.	EN short to R _{ISET} removed.
Thermal Shutdown	Off	The die temperature exceeds 165°C	The die temperature cools down below 140°C. FAULTB pin recovers immediately.

LAYOUT CONSIDERATIONS

As for all switching power supplies, especially those providing high current and using high switching frequencies, layout is an important design step. If layout is not carefully done, the operation could show instability as well as EMI problems.

The high dV/dt surface and dI/dt loops are big noise emission source. To optimize the EMI performance, keep the area size of all high switching frequency points with high voltage compact. Meantime, keep all traces carrying high current as short as possible to minimize the loops.

- (1) Wide traces should be used for connection of the high current paths that helps to achieve better efficiency and EMI performance. Such as the traces of power supply, inductor L₁, current recirculating diode D₁, LED load and ground.
- (2) Keep the traces of the switching points shorter. The inductor L₁, LX and current recirculating diode D₁ should be placed as close to each other as possible and the traces of connection between them should be as short and wide as possible.
- (3) To avoid the ground jitter, the components of parameter setting, R_{ISET}, should be placed close to the device and keep the traces length to the device pins as short as possible. On the other side, to prevent the noise coupling, the traces of R_{ISET} should either be far away or be isolated from

high-current paths and high-speed switching nodes. These practices are essential for better accuracy and stability.

- (4) The capacitor C_{IN} should be placed as close as possible to VCC pin for good filtering.
- (5) Place the bootstrap capacitor C_{BOOT} close to BOOT pin and LX pin to ensure the traces as short as possible.
- (6) The connection to the LED string should be kept short to minimize radiated emission. In practice, if the LED string is far away from the driver board, an output capacitor is recommended to be used and placed on driver board to reduce the current ripple in the connecting wire.
- (7) The thermal pad on the back of device package must be soldered to a sufficient size of copper ground plane with sufficient vias to conduct the heat to opposite side PCB for adequate cooling.

THERMAL CONSIDERATIONS

The package thermal resistance, θ_{JA} , determines the amount of heat that can pass from the silicon die to the surrounding ambient environment. The θ_{JA} is a measure of the temperature rise created by power dissipation and is usually measured in degree Celsius per watt (°C/W).

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When operating the chip at high ambient temperatures, or when driving maximum load current, care must be taken to avoid exceeding the package power dissipation limits. The maximum power dissipation can be calculated using the following Equation (20):

$$P_{D(MAX)} = \frac{T_{J(MAX)} - T_A}{\theta_{JA}} \quad (20)$$

Where $T_{J(MAX)}$ is the recommended maximum operating junction temperature.

So,
$$P_{D(MAX)} = \frac{125^{\circ}\text{C} - 25^{\circ}\text{C}}{42.7^{\circ}\text{C/W}} \approx 2.34\text{W}$$

Figure 40, shows the power derating of the IS32LT3953B on a JEDEC boards (in accordance with JESD 51-5 and JESD 51-7) standing in still air.

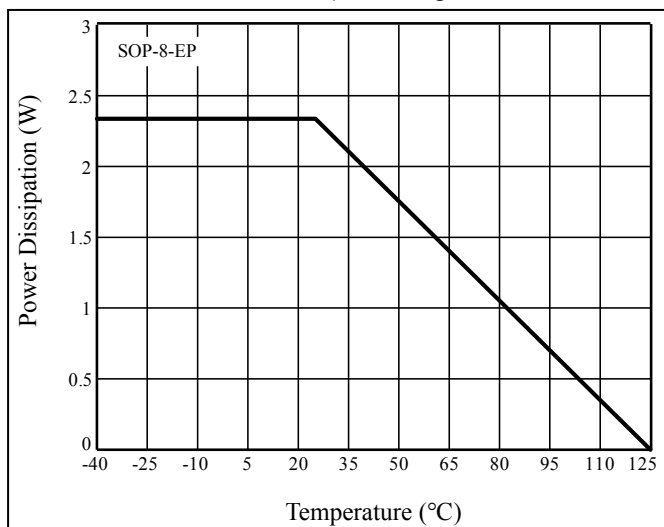


Figure 40 Dissipation Curve

The thermal resistance is achieved by mounting the IS32LT3953B on a standard FR4 double-sided printed circuit board (PCB) with a copper area of a few square inches on each side of the board under the IS32LT3953B. Multiple thermal vias, as shown in Figure 41, help to conduct the heat from the exposed pad of the IS32LT3953B to the copper on each side of the board. The thermal resistance can be reduced by using a metal substrate or by adding a heatsink.

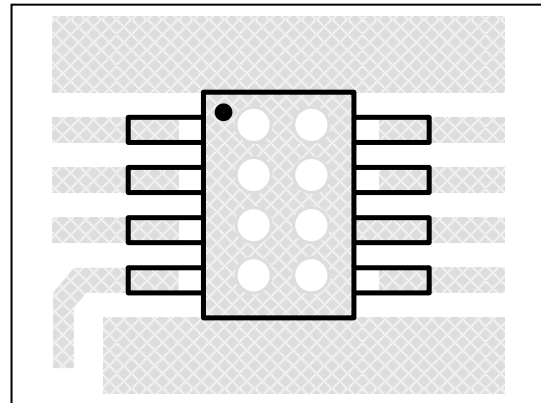


Figure 41 Board Via Layout For Thermal Dissipation

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CLASSIFICATION REFLOW PROFILES

Profile Feature	Pb-Free Assembly
Preheat & Soak Temperature min (T _{smin}) Temperature max (T _{smax}) Time (T _{smin} to T _{smax}) (t _s)	150°C 200°C 60-120 seconds
Average ramp-up rate (T _{smax} to T _p)	3°C/second max.
Liquidous temperature (T _L) Time at liquidous (t _L)	217°C 60-150 seconds
Peak package body temperature (T _p)*	Max 260°C
Time (t _p)** within 5°C of the specified classification temperature (T _c)	Max 30 seconds
Average ramp-down rate (T _p to T _{smax})	6°C/second max.
Time 25°C to peak temperature	8 minutes max.

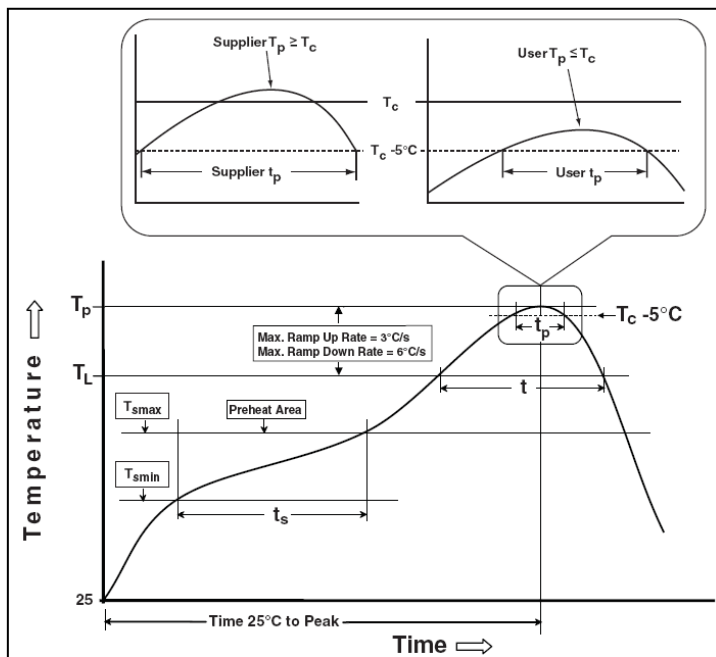
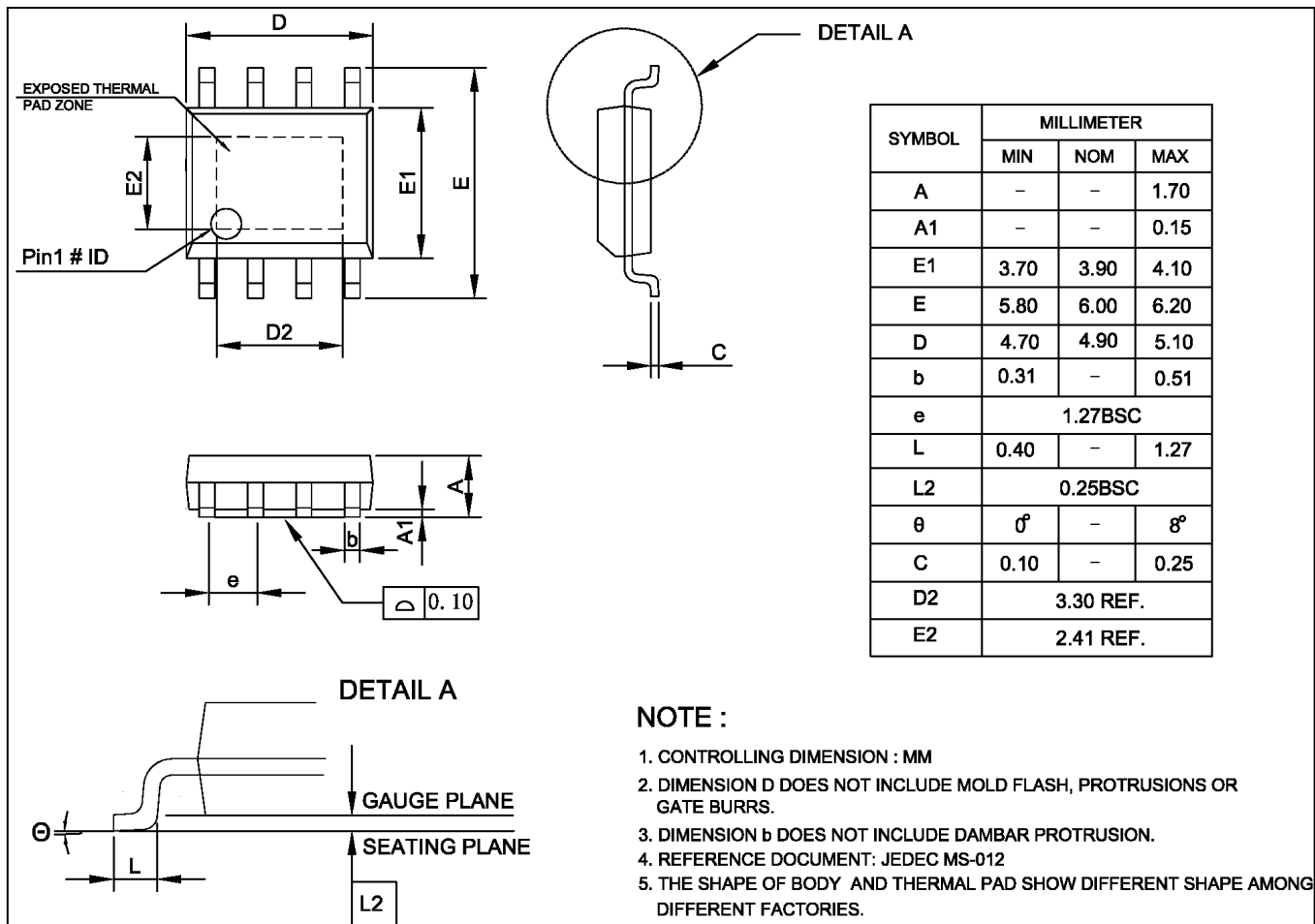


Figure 42 Classification Profile

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PACKAGE INFORMATION

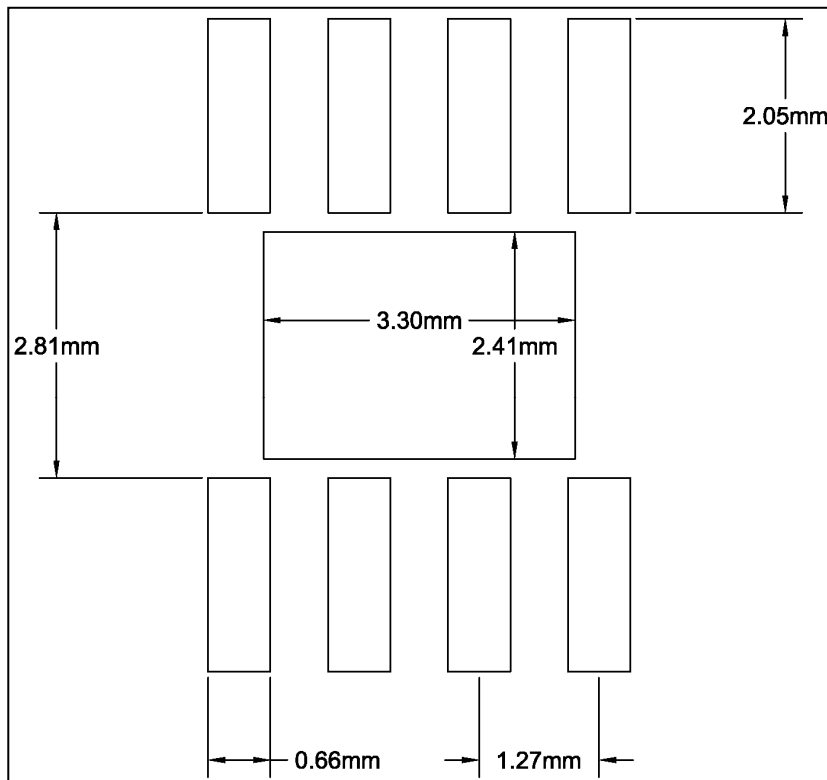
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RECOMMENDED LAND PATTERN

SOP-8-EP



Note:

1. Land pattern complies to IPC-7351.
2. All dimensions in MM.
3. This document (including dimensions, notes & specs) is a recommendation based on typical circuit board manufacturing parameters. Since land pattern design depends on many factors unknown (eg. user's board manufacturing specs), user must determine suitability for use.

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REVISION HISTORY

Revision	Detail Information	Date
0A	Initial release	2020.01.15
A	Update EC and release to final version	2020.04.20
B	Remove IDD_LIM maximum value in EC	2020.06.20